S. PHROMPICHAI, SGD FREQUENCY-DOMAIN SPACE-FREQUENCY SEMIBLIND MULTIUSER RECEIVER ...
in [12]. This technique offers space and frequency diversity over multi-antenna and frequency-selective fading channels. As appeared in [12], [13], the SFBC using code division multiplexing (CDM) in OFDM system has better performance and is more robust than STBC OFDM system.

Blind multiuser detection and channel estimation receivers based on subspace decomposition are proposed in [14-16]. Blind receivers appear more attractive than the non-blind counterparts, i.e., the training-based ones since the bandwidth and power are not consumed by the training signals. However, the blind algorithms require a long duration of observation and often result in a phase ambiguity in the estimate. Moreover, the channel is required to be time invariant during a long period. For STBC based on Alamouti’s scheme [8] in frequency-selective fading channel, it is impossible to achieve blind receiver due to implicit ambiguity [9]. Therefore, in practice of the blind algorithms for very high data rate future mobile wireless communication systems are limited unless these drawbacks are alleviated.

The pilot (training) signal and multiuser signal are together transmitted in parallel, which is called the common pilot channel (CPICH) as a standard for 3rd Generation Partnership Project 2 (3GPP2) mobile communication systems [17]. This technique is very beneficial for the multiuser receiver to track fast time-varying multipath channel information in order to detect the desired user data and suppress interferences.

Recently, the semiblind receiver has been gaining interest for high data rate mobile wireless communication systems. The criterion of a semiblind receiver combines information of both known (pilot) and unknown (estimating) data signals for tracking channel and suppressing ISI. It has been proven in [18], [19], that this technique provides superior performance over blind or pilot-based ones. An optimal linear semiblind receiver in the form of minimum mean square error (MMSE) [20] and the semiblind channel estimation using the exact maximum-likelihood estimate receiver [21] were proposed for downlink systems. These techniques achieve a reasonable trade-off between performance and typically prohibitive large complexity. A suboptimal semiblind space-frequency (SF) multiuser detection [22], semiblind channel estimation [23], and semiblind multiuser receiver [11] presented a method based on subspace decomposition. These schemes are batch-processing and employed in scenarios where the pilot and unknown data do not overlap in time.

Frequency domain equalizer (FDE) has been shown to be an attractive scheme for wireless systems with frequency-selective fading channel. Compared with the time-domain equalizer (TDE), FDE has less computational complexity and better convergence property [24]. The linear FDE channel estimation for multiple-input multiple-output (MIMO) downlink systems based on least square (LS) and MMSE criteria were proposed in [25-28]. The FDE multiuser receivers [29], [30] were proposed for MIMO-CDMA systems with CPICH in frequency selective-fading channel. The FDE semiblind channel estimation using data energy besides pilot signal energy was proposed for 3GPP LTE uplink systems [31]. These schemes can be operated in the maximum multi-antenna diversity, maximum multipath diversity and multiuser communication scheme. In addition, the receivers are designed to act on each per-tone basis in FD and require the estimation from the inverse matrices. Therefore, the overall computational complexity increases relatively with number of used frequency tones in the systems and the length of filter weight vector.

Least-mean-square (LMS) type adaptive receivers are attractive due to their very low computational complexity. The fast convergence FD training-based LMS adaptive multiuser receiver for STBC MC-CDMA systems was proposed in [32]. The updated weight vector relies on the relationship between two mean-square errors (MSE) from odd and even indexes. The FD LMS adaptive decision feedback equalizer [33] and the variable step-size based LMS channel estimation algorithm [34] were proposed for single carrier systems. However, these methodologies are designed to operate on systems with sufficient CP and have not been applied with CPICH systems. Moreover, these techniques suffer from the problem of signal to interference plus noise ratio (SINR) drop resulting from the use of a shared equalizer in the detection of the desired user data.

In this paper, we propose a novel methodology to improve the performance of FD semiblind multiuser receivers with a fixed mixing parameter by using an adaptive optimal mixing parameter. The mixing parameter plays a key role to control the mixing information ratio between blind-based and training-based modes with various amounts of active loaded users existing in the systems.

The contributions of this paper are as follows: First, a mathematical framework of a synchronous SFBC downlink MIMO MC-CDMA with CPICH and without CP signal model is presented, and matrix for using the advantage of diversity from SF technique and array antennas is for-
mulated. Second, the suboptimal FD SF semiblind multiuser receiver with mixing parameter is considered. The optimal mixing parameter is analytically addressed. Third, to reduce computational complexity, the stochastic gradient descent (SGD) FD SF semiblind multiuser receiver with adaptive parameters is proposed.

Computer simulation results show that the proposed semiblind receiver outperforms existing adaptive step-size (AS) LMS semiblind with fixed mixing parameter and conventional AS-LMS training-based multiuser receivers in MSE, symbol error rate (SER) and SINR in both static and dynamic channel models.

1.1 Notation

In this paper, we use bold lower case for vectors and bold upper case for matrices. Also, * is convolution operation, (·)T for transpose, (·)H for Hermitian matrix, (·)* for complex conjugate, (·)† for inverse matrix and [·] denotes rounding up to the nearest integer. Throughout this paper, receiver, equalizer and algorithm convey the same meaning and are used interchangeably.

2. SFBC Downlink MIMO MC-CDMA with CPICH System

Let us consider a baseband model for SFBC downlink MIMO MC-CDMA with CPICH and without CP system which is illustrated in Fig. 1. For conciseness, we will focus on a base station (BS) with two transmit antennas and a mobile with two receive antennas, where the base station has K symbol-synchronous active users existing in the systems. The kth mobile user is assigned an orthogonal chip signal sequence (tj), where kj = 0 reserved for the pilot signal. Following this, the signals from all users, including the pilot, are combined. Hence, a synchronous code division multiplexed signal tm is given by

\[ t(m) = Cx(m) \]  

where \( x(m) = [\sqrt{A_0(m)h_0(m)}, \ldots, \sqrt{A_N(m)h_N(m)}]^T \), \( A_k(m) \) and \( h_k(m) \) are power and data symbol for kth user, m is symbol sequence, \( C = [c_0, \ldots, c_L] \) and \( c_k = [c_{k,0}, \ldots, c_{k,N-1}] \) are complex spreading code matrix and vector, respectively. The complex transmit multiuser signal tm is stored for two symbols (data block) and loaded into the SFBC encoder for using the diversity from SF and MIMO techniques which is based on the STBC Alamouti’s scheme [8, 12]

\[
\begin{bmatrix}
    t_0(2j) & t_0(2j+1) \\
    t_1(2j) & t_1(2j+1)
\end{bmatrix}
\]  

where

\[
t_0(2j) = [t(2(j-1)N), \ldots, t(2(j-1)N + N - 1)],
\]

\[
t_1(2j) = [t(2(j-1)N + N), \ldots, t(2(j-1)N + 2N - 1)],
\]

and

\[
t_k(2j+1) = -t^*_k(2j)P_N, \quad t_k(2j+1) = t^*_k(2j)P_N.
\]

where \( j \) is block sequence and \( P_N \) is an \( N \times N \) permutation matrix that performs a reversal of the entries. The complex transmit multiuser signals, even \( t_{u_e}(2j) \) and odd \( t_{u_o}(2j+1) \) block signal sequences, are loaded into the OFDM modulators using the inverse discrete Fourier transform (IDFT). It is assumed that the number of subcarriers is equal to the processing gain of the spreading code.

\[
\hat{r}_{u_e}(j) = \text{IDFT}(t_{u_e}(j)),
\]

\[
= [\hat{r}_{u_e}(0), \ldots, \hat{r}_{u_e}(N-1)].
\]

where \( M_f = 1, 2 \) is the index of the transmit antenna. After modulation, the complex FD transmit multiuser encoding signal \( t_{u_e}(j) \) is transformed to the complex TD transmit multiuser encoding signal \( \hat{r}_{u_e}(j) \). Finally, the complex TD encoding multiuser block signal both even \( \hat{r}_{u_e}(2j) \) and odd \( \hat{r}_{u_o}(2j+1) \) sequences are loaded into parallel-to-series converter, multiplied by a cell-specific long scrambling code sequence \( s(i) \) and transmit at the \( M_f^n \) transmit antenna

\[
\hat{u}_{u_e}(i) = \hat{r}_{u_e}(i) \times s(i)
\]

where \( i \) is chip rate index. The signal from BS propagates through MIMO multipath frequency-selective fading channel. Here, the channel is modeled as a finite impulse response (FIR) filter with complex channel impulse response \( h_{u_e}(i,l), l \in \{0, \ldots, L_0\} \), where \( L_0 \) is order of channel. The received signal at the mobile station (MS) antenna is then the convolutional result of transmit signal and MIMO channel impulse response plus corrupted additive white Gaussian noise (AWGN), i.e.

\[
\hat{r}_{u_e}(i) = \hat{u}_{u_e}(i) * \hat{h}_{u_e}(i) + \hat{w}(i),
\]

\[
\hat{r}_{u_o}(i) = \hat{u}_{u_o}(i) * \hat{h}_{u_o}(i) + \hat{w}(i)
\]

where \( \hat{u}_{u_e}(i) \) is complex AWGN with mean 0 and variance \( \sigma^2_w \), and \( M_f = 1, 2 \) is the index of the receive antenna.

At the receiver, the complex TD received multiuser chip signal sequence \( \hat{r}_{u_e}(i) \) is descrambled by the cell-specific long scrambling code \( s(i) \), then stored for two symbols, transformed information to FD using OFDM demodulators and loaded into SFBC decoder. To obtain the advantage of diversity from SFBC technique and array antennas, the \( L_0 \times N \) complex FD received multiuser shifted block signal sequence matrix \( R(j) \) is compactly formulated as

\[
R(j) = F^H_N \left( \tilde{H}(j) + \tilde{W}(j) \right)^H,
\]
where $F_N$ is a sliding FFT [35], $W$ is an AWGN matrix and

$$
\mathbf{\hat{H}}(j) = \begin{bmatrix}
\mathbf{\hat{H}}_1(j) \\
\mathbf{\hat{H}}_2(j) \\
\mathbf{\hat{H}}_3(j) \\
\mathbf{\hat{H}}_4(j)
\end{bmatrix}
$$

(9)

where

$$
\mathbf{\hat{h}}_{M_1r}(j) = \begin{bmatrix}
\mathbf{\hat{h}}_{M_1r}(L_0) & \cdots & \mathbf{\hat{h}}_{M_1r}(0) & 0_{2^1} & \cdots & 0_{2^1} \\
0_{2^1} & \cdots & \mathbf{\hat{h}}_{M_1r}(L_0) & \cdots & \mathbf{\hat{h}}_{M_1r}(0) & \cdots & \mathbf{\hat{h}}_{M_1r}(L_0) \\
0_{2^1} & \cdots & 0_{2^1} & \cdots & \mathbf{\hat{h}}_{M_1r}(L_0) & \cdots & \mathbf{\hat{h}}_{M_1r}(0)
\end{bmatrix}
$$

(10)

and

$$
\bar{t}(j) = \begin{bmatrix}
\bar{t}_1(j) \\
\bar{t}_2(j)
\end{bmatrix}
$$

(12)

where

$$
\mathbf{\hat{t}}_k(j) = \begin{bmatrix}
\hat{t}_k(2N-L_k + L_k + 1) \\
\cdots \\
\hat{t}_k(L_k) \\
\hat{t}_k(2N-L_k + L_k + 1)
\end{bmatrix}
$$

and $L_j$ denotes length of the equalizer which is selected.

3. FD SF Multiuser Receivers

In this section, a theoretical FD SF multiuser-trained MMSE receiver is presented. A suboptimal FD SF semi-blind multiuser receiver with mixing parameter is considered, and the solution obtained optimal mixing parameter is derived. Finally, an SGD FD SF semiblind multiuser receiver with adaptive parameters is proposed to reduce the computational complexity.

3.1 FD SF Multiuser-trained MMSE Receiver

A theoretical FD SF multiuser-trained MMSE equalizer obtained by minimizing the MSE criterion is considered. The advantage of diversity from SFBC technique and array antennas passing the complex FD received multiuser shifted block signal sequence matrix $R(j)$ are used to update algorithms. For conciseness, FD SF multiuser-trained MMSE cost function in odd and even parts are formulated as

$$
J_{\text{MMSE}} = \mathbf{E}[\mathbf{f}_{\text{MMSE}}^*(j)R(j) - t_v(j)]
$$

(14)

where $t_v = [0, \ldots, 0, t_v, 0, \ldots, 0]$ is complex synchronous FD SF multiuser training signal for subcarrier $v$.

For supporting (14), we assume that the receiver knows the complex synchronous FD SF multiuser training signal $t(j)$. It is an independent and identically distributed (i.i.d.) random variable with zero mean and unit variance. Hence, the updated equation of FD SF multiuser-trained MMSE equalizer is given as (see Appendix A.)

$$
f_{\text{MMSE}} = \frac{\sigma_v^2}{N} (\mathbf{\hat{h}}_v^H + \sigma_n^2 I) \mathbf{\hat{h}}_v
$$

(15)

where $k_v = [0, \ldots, 0, 1, 0, \ldots, 0]$ is unit vector with one in $v$ position, $\sigma_v^2$ noise power and $\sigma_n^2$ denotes total received signal power with $K$ active loaded users existing in the systems.

$$
\sigma_v^2 = A_0 + \sum_{k=1}^{K} A_k
$$

To obtain the updated optimal tap-weight equalizer, the receiver requires to perfectly know the complex FD channel response, total received signal power and noise power.

3.2 FD SF Semiblind Multiuser Receiver with Mixing Parameter

In practical use, transmission complex synchronous FD SF multiuser training signal $t(j)$ obtained $f_{\text{MMSE}}$ wastes bandwidth and power efficiencies, and increases the system’s complexity. Blind multiuser receivers are impractical for multipath frequency-selective fading channel. Moreover, blind and training-based receivers suffer from degraded performance in fast time varying fading channel compared to semiblind receivers. Therefore, the algorithm uses the advantage of transmit pilot signal parallel with data signals channel [17] is considered in this subsection. The suboptimal FD SF semiblind multiuser receiver with optimal mixing parameter is considered to improve the performance of FD semiblind multiuser receiver with fixed mixing parameters, which reduces the computational complexity of optimal linear FD semiblind receivers and optimal FD SF multiuser-trained MMSE receiver. The algo-
rithm exploits the methodology of adapted mixing information ratio between training-based mode and blind-based mode.

To formulate the suboptimal algorithm, MSE cost function consisting of the blind-based and the training-based (non-blind) parts is given as

\[ J(f, \phi) = E \left[ \phi \left| v_d(j) \right|_{\text{blind}}^2 + (1 - \phi) \left| v_p(j) \right|_{\text{training-based}}^2 \right] \]

where

\[ e_d(j) = (T^H \gamma_d - \hat{b}_d(j)) \]
\[ e_p(j) = (T^H \gamma_p - \hat{b}_p(j)) \]

where \( \gamma_d = R(j)e_d \), \( \gamma_p = R(j)e_p \), \( \phi \) is a mixing parameter, \( \hat{b}_d(j) \) pilot data symbol block sequence, \( \hat{b}_p(j) \) estimated data symbol block sequence of the desired user \( \left( \hat{b}_d(j) = (T^H(j)\gamma_d) \right) \), \( e_d \) complex FD desired user spreading code vector and \( e_p \) is complex FD pilot spreading code vector.

For supporting the operation in very high data rate downlink MIMO MC-CDMA systems with multipath frequency-selective fading channel in which amplitude, phase and tapped delay of channel are varied with time. Moreover, tapped delay of channel is large delay spread over symbol block. Therefore, information from all subcarriers \( (1,\ldots,G) \) or group are used to update the tap-weight coefficients vector of the equalizer passing the formulated complex FD received multiuser shifted block signal sequence matrix \( R(j) \). As a result, the suboptimal algorithm can be operated in either system with sufficient CP, insufficient CP or even without CP.

Assuming that the suboptimal receiver perfectly knows the complex FD desired user code \( e_d \) and pilot code \( e_p \) vectors. Hence, the updated equation of FD SF semiblind multiuser equalizer with mixing parameter is obtained as (see Appendix B.)

\[ f = (A_p - \phi(A_p + A_d)) \left( \sigma^2_N H H^H + \sigma^2_N I \right)^{\dagger} H_i. \]  

(19)

3.3 Optimal Mixing Parameter

Considering (17), performance of the suboptimal semiblind multiuser receiver relies upon the mixing parameter \( \phi \). Hence, the methodology obtained the optimal mixing parameter which is based on the following assumption:

- If mixing parameter \( \phi \) is appropriately chosen, our FD SF semiblind multiuser with mixing parameter equalizer coincides with the theoretical FD SF multiuser-trained MMSE equalizer.

Since, the optimal mixing parameter is verified by setting (19) equal (15), i.e. \( f = f_{\text{MMSE}} \)

\[ \frac{\sigma^2_N}{N} \left( \sigma^2_N H H^H + \sigma^2_N I \right)^{\dagger} H_i, \]

(20)

The suboptimal FD SF semiblind multiuser receiver with mixing parameter coincides with the FD SF multiuser-trained MMSE receiver, if and only if

\[ A_p - \phi(A_p + A_d) = \frac{\sigma^2_N}{N} \]

(21)

hence, the optimal mixing parameter \( \phi_{\text{opt}} \) is finally obtained as

\[ \phi_{\text{opt}} = \left( \frac{A_p}{A_p + A_d} \right) \]

(22)

where \( A_d \) is the received desire user power and \( A_p \) is the received pilot power, respectively.

From (22), we found that the optimal mixing parameter relies upon the power of each user and the number of active loaded users existing in the systems.

3.4 SGD FD SF Semiblind Multiuser Receiver with Adaptive Optimal Mixing Parameters

The SGD FD SF semiblind multiuser receiver based on the methodology of adaptive optimal parameters is proposed to improve performance of the FD SF semiblind multiuser receivers with fixed mixing parameter, and reduce the computational complexity of suboptimal FD SF semiblind multiuser receivers and suboptimal FD SF semiblind multiuser receiver with mixing parameter. Moreover, it increases the ability in tracking fast time varying multipath frequency-selective fading channel in SFBC downlink MIMO MC-CDMA with CPICH and without CP systems.

Applying a standard SGD method into (17), the adaptation for SGD FD SF semiblind multiuser equalizer tap-weight coefficients vector \( \hat{R}(j) \) at \( j^{th} \) even and odd block sequence using LMS algorithm is obtained as

\[ f(j + 1) = f(j) - \mu \left( \phi(j) \epsilon_j (j) \gamma_d + (1 - \phi(j)) \epsilon_j \gamma_p \right). \]

(23)

The SGD FD SF equalizer is employed to counter the effective multipath frequency-selective fading channels, restore the orthogonality of the user’s spreading code signal and suppress MUI. However, performance of the SGD FD SF equalizer heavily depends on mixing parameter and a choice of step-size. Hence, the adaptive mixing parameter and the adaptive step-size [36] are incorporated in the semiblind updated function.

Referring to (22), to obtain the optimal mixing information ratio between the blind-based mode and the train-
ing-based mode, the receiver requires knowledge of the received signal power of pilot and desired user, and active loaded users existing in the systems which increase the computational complexity of the receiver. Hence, the automatically adaptive optimal mixing parameter using LMS algorithm is proposed. The adaptive mixing parameter at each recursion $j$, $\phi(j)$ is updated in order to minimize

$$J(f, \phi) = \left[ \begin{array}{c} e_j(f) + p_j(f) \end{array} \right]^{\mu+}$$

$$\phi(j+1) = \phi(j) - \beta \left( \frac{\partial J(f, \phi)}{\partial \phi} \right)_{\phi = \phi(j)}$$

(24)

where $\beta$ denotes as an adaptation parameter for the adaptive mixing parameter part and $[\star]_{\mu-\mu+}$ is truncation to the lower and upper mixing parameter limits. The derivative $\Psi(j)$ representing $\frac{\partial J}{\partial \phi}$ is updated as

$$\Psi(j+1) = \left[ 1 + \mu(j) \left( \frac{\phi(j)\Psi_{d,j} + \Psi_{s,j}}{\phi(j)\Psi_{d,j} + \Psi_{s,j}} \right) \right] \Psi(j)$$

$$- \mu(j) \left( e_j(j)\Psi_{d,j} - e_j(j)\Psi_{s,j} \right)$$

(25)

where $\Psi_{d,j} = \gamma_{d,j}^{\mu+}$ and $\Psi_{s,j} = \gamma_{s,j}^{\mu+}$.

However, the performance of the SGD FD SF semiblind multiuser receiver is heavily dependent on the choice of step-size. Hence, the AS-LMS algorithm is incorporated which in turn improves the performance of the receiver in a dynamic channel where the number of interference users in the system is time-varying. The receiver automatically adapts the step-size by minimizing the mean square error output. Subsequently, the AS-LMS scheme at each recursion $j$, $\mu(j)$ is updated using the gradient obtained by minimizing the MSE cost $J(f, \phi)$ with respect to the step-size $\mu$ , $\frac{\partial J(f, \phi)}{\partial \mu} = \mu_{-\mu+j}$

$$\mu(j+1) = \left[ \mu(j) - \alpha \left( \frac{\phi(j)\Psi_{d,j} + \Psi_{s,j}}{\phi(j)\Psi_{d,j} + \Psi_{s,j}} \right) \right]^{\mu-\mu}$$

(26)

where $\alpha$ denotes as an adaptation parameter for the AS part and $[\star]_{\mu-\mu+}$ is the truncation to the lower and upper step-size limits. The derivative $q(j+1)$ represents $\frac{\partial J}{\partial \mu}$ and is adapted according to

$$q(j+1) = \left[ 1 - \mu(j) \left( \frac{\phi(j)\Psi_{d,j} + \Psi_{s,j}}{\phi(j)\Psi_{d,j} + \Psi_{s,j}} \right) \right] q(j)$$

$$- \left( \frac{\phi(j)e_j(j)\Psi_{d,j} + \Psi_{s,j}}{\phi(j)e_j(j)\Psi_{d,j} + \Psi_{s,j}} \right)$$

(27)

Finally, estimated data symbol of the desired user at $\ell^d (2j+1)$ and even $(2j)$ block sequences can be directly detected as

$$\hat{b}_d (2j+1) = f_j (2j+1)\gamma_d ,$$

$$\hat{b}_d (2j) = f_j (2j)\gamma_d .$$

(28)

The computational complexity of the SGD FD SF semiblind multiuser receiver with adaptive parameters is investigated in this subsection. The receiver involves three LMS algorithms in 1) adapting the FD SF tap-weight coefficients vector, 2) adapting optimal mixing parameter, and 3) adapting optimal step-size. For updated odd and even tap-weight equalizers through (23)-(27), where each of these adaptive LMS algorithms have computational complexity in order of $O(N)$ [37-38]. Therefore, the proposed SGD FD SF semiblind multiuser receiver possesses computational complex is $O(N)$ whereas suboptimal FD receivers incur minimum computational complex are $O(N^2)$. Furthermore, the proposed SGD FD SF semiblind multiuser receiver with adaptive optimal mixing parameter has a less increasing rate of computational complexity than those of conventional FD SF AS-LMS training-based receivers and FD SF AS-LMS semiblind multiuser with fixed mixing parameter receivers, whose computational complexities are $O(N)$.

4. System Parameters

The system parameters were derived according to an outdoor propagation scenario. We used a link level MIMO channel model which had been specifically developed within the Multi Element Transmit Receive Antennas (METRA) model for Mobile Broadband Wireless Access (MBWA) system MIMO channel project [39]. This channel model was based on 3GPP/3GPP2 proposal [17] for mobile broadband wireless MIMO channel exploiting multipath angular characteristics. It consists of elaborating a spatial model from the hybrid approach between a geometrical concept depending on cluster position and the tapped delay line model describing the average power delay profile with a fixed number of taps. The spatial parameters were defined at the BS and at MS. The angular distribution was modeled from parameters leading to an average of angle spread [40].

The Case B ITU Pedestrian A MIMO channel parameters with 0.5\textdegree\ antenna spacing, uniform power azimuth spectrum (PAS) and angle of arrival (AOA) 22 degree was considered. The classical Rayleigh model was used to generate the uncorrelated fading signal. We used 3GPP2 MIMO channel power delay profile with a fixed number of taps [17] to model an outdoor environment which was characterized by a large delay spread, a higher mobility and a symmetrical antenna configuration.

We considered the system which was based on a sampling frequency 57.6 MHz with a carrier frequency of
5 GHz and the subcarriers equaled spreading code. The complex orthogonal FD spreading codes were employed as the user-specific code which had the length $N = 32$. The BS transmits QPSK symbol and all users had the same powers. The transmit power at antenna one and antenna two were normalized to one. The additive noise was an AWGN.

In simulation, MIMO radio channels were inserted between transmit and receive antennas of the SFBC downlink MIMO MC-CDMA system model. Besides, the correlation properties in the spatial domain of the broadband wireless MIMO channel were obtained from the Kronecker product of two independent correlation matrices which were defined by the correlation properties at the BS and MS and the associated Doppler spectrum of the channel part.

5. Simulation Results

The performance of adaptive FD SF multiuser receivers were investigated, the proposed SGD semiblind multiuser receiver with adaptive optimal mixing parameter was compared with the conventional AS-LMS training-based, the AS-LMS semiblind with fixed mixing parameter $\phi_{\text{fixed}} = 0.1$, and the theoretical multiuser-trained MMSE receivers in SFBC downlink MIMO MC-CDMA with CPICH and without CP system under fast time varying multipath frequency-selective fading channels. The fixed mixing parameter $\phi_{\text{fixed}} = 0.1$ based on an optimal value which was proposed in [29]. The MIMO channel model was set based on the 3GPP2 modified Pedestrian A with a Doppler speed of 120 km/h.

The proposed semiblind and AS-LMS semiblind with fixed mixing parameter receivers assumed knowledge of the pilot and desired user code vectors. The AS-LMS training-based receiver assumed only knowledge of the pilot code vector. Theoretical multiuser-trained MMSE receiver assumed perfect knowledge of complex FD channel response, total received signal power and noise power, and updated using LS method with inverse matrix term.

We assumed throughout this section that the first user ($k = 1$) is the desired user. An initial step-size as $\mu_{0}$ for the AS-LMS algorithms were chosen $\mu_{0} = 1 \times 10^{-3}$. The upper and lower step-size limits $\mu^{+}$ and $\mu^{-}$ were 0.5 and 0, respectively. Also, the adaptation factors $\alpha$ of $1 \times 10^{-2}$ and $\beta$ of $1 \times 10^{-4}$ were selected. The initial mixing parameter $\phi_{0}$ for the proposed algorithm was chosen as $\phi_{0} = 0.15$ and the upper and lower mixing parameter limits $\phi^{+}$ and $\phi^{-}$ were 1 and 0, respectively. All receivers used the same order of equalizer $L_f = 31$ and updated at block size. The static and dynamic environments were investigated in this section.

5.1 Static Environments

A system consisting of the pilot ($k = 0$), desired user ($k = 1$) and various amounts (2, 14 and 30) of equal power interfering users was considered. Fig. 2(a) illustrates an averaged MSE attaining from the proposed semiblind, AS-LMS semiblind with fixed mixing parameter, AS-LMS training-based and multiuser-trained MMSE algorithms at 4, 16 and 32 active loaded users existing in the system. The MSE value of the proposed semiblind algorithm at the steady state is lower than the AS-LMS semiblind with fixed mixing parameter and training-based algorithms in the case of 4 and 16 active loaded users existing in the system.
16 and 32 active loaded users existing in the system, the mixing parameter values from the proposed algorithm adapt closely to the optimal mixing parameter value.

Fig. 3 illustrates an averaged SER attaining from all algorithms where SNR = 10 dB was set. At SER = $1 \times 10^{-4}$ in the case of half-loaded users ($K = 15$), the proposed semiblind algorithm achieves an improvement in reducing the transmit power approximately 1.1 dB and 2 dB over the AS-LMS semiblind with fixed mixing parameter and AS-LMS training-based algorithms, respectively. Moreover, we observe that the difference in the performance between the proposed semiblind, AS-LMS semiblind with fixed mixing parameter and AS-LMS training-based algorithms decreases where the number of active loaded users existing in the system increases. This consistency with the predicted optimal mixing parameter value (22) and simulation result is shown in Fig. 2. Thus, it can be explained that the semiblind algorithms depend on less information from the blind-based mode where the number of active loaded users existing in the system increases. Considering the case of full-loaded users ($K = 31$), the mixing parameter adapts towards zero (Fig. 2(b)) and the predicted optimal mixing parameter value equals zero ($\phi_{\text{opt}} = 0$). As a result, the semiblind algorithms converge to fully utilize information from training-based mode only. Clearly, the semiblind algorithms have the same performance as the training-based algorithm.

In this subsection, it is clear that the performance of semiblind algorithm has an improvement when the mixing ratio of information between blind-based mode and training-based mode is adapted to an optimal value.

5.2 Dynamic Environments

This simulation compares the tracking capability of each receiver in detection of the desired user in a dynamic environment where the number of active loaded users existing in the system changes abruptly. Simulation parameters were identical to the static environment case. At initial block time $j = 0$, pilot ($k = 0$), desired user ($k = 1$) and 14 interference users ($k = 2, \ldots, 15$) were activated in the system. At $j = 600$, 12 interfering users ($k = 4, \ldots, 15$) exited from the system. At $j = 1200$, 28 interfering users ($k = 4, \ldots, 31$) entered the system. Fig. 5(a) illustrates the averaged SINR. The proposed semiblind algorithm responds to the abrupt change in the number of active loaded users. It offers SINR improvement of approximately 1 dB and 0.7 dB in the weak-loaded users, 0.5 dB and 0.3 dB in the half-loaded users, in detection of the desired user over AS-LMS training-based and AS-LMS semiblind with fixed mixing parameter algorithms, respectively. It is clear that the proposed semiblind multiuser with adaptive mixing parameter algorithm can suppress more interference users than existing algorithms. Fig. 5(b) shows the averaged step-size and the adaptive mixing parameter trajectories of the proposed semiblind algorithm. For a sudden change, the trajectories of the step-size and the mixing parameter adapt closely to the optimal values result of the receiver incorporating the adaptive mixing parameter and the AS-LMS. Furthermore, the semiblind algorithms mitigate the problem of SINR drop resulting from the use of a shared equalizer to detect the desired user as found in over existing conventional LMS training-based algorithm.
In summary, incorporating the adaptive optimal mixing parameter into a semiblind algorithm can improve performance of the semiblind with fixed mixing parameter receiver in both dynamic and static environments.

6. Conclusions

The analytical results in this paper show that the optimal mixing information ratio between blind-based mode and training-based mode of semiblind multiuser receivers relies on power and number of active loaded users existing in the systems. The SGD FD SF semiblind multiuser receiver with adaptive optimal mixing parameter has been proposed to improve performance of the semiblind multiuser receivers with fixed mixing parameter and to reduce computational complexity of the suboptimal semiblind multiuser receivers for SFBC downlink MIMO MC-CDMA with CPICH systems in multipath frequency-selective fading channel. The simulation results reveal that performance of the proposed receiver outperforms the existing FD SF semiblind with fixed mixing parameter and the conventional FD SF training-based multiuser receivers in MSE and SER. Moreover, the proposed receiver has an improvement in the SINR over existing FD SF multiuser receivers in a dynamic environment where the number of active loaded users existing in the system is changes abruptly.

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Appendix A: Derivation of the FD SF Multiuser-trained MMSE Equalizer

Substituting (8) into optimal multiuser-trained MMSE cost function (14) and taking the expectation, we obtain

\[ J(f_{\text{MMSE}}) = \mathbb{E} \left( f_{\text{MMSE}}^H \left( \mathbf{H}^H (\mathbf{I} + \mathbf{W}^H \mathbf{W}) f_{\text{MMSE}} \right) \right) \]

Taking the gradient of (A.1) with respect to \( f_{\text{MMSE}} \) and setting the result to zero gives us

\[ \nabla f_{\text{MMSE}} J_{\text{MMSE}} = (\sigma^2 \mathbf{I} + \sigma^2_1) f_{\text{MMSE}} - \frac{\sigma^2}{N} \mathbf{H}_i = 0 \quad \text{(A.2)} \]

where \( \mathbf{H} = \mathbf{F} \left( \mathbf{H} \right) \). Solving for \( f_{\text{MMSE}} \) we obtain

\[ f_{\text{MMSE}} = \frac{\sigma^2}{N} \left( \sigma^2 \mathbf{I} + \sigma^2_1 \mathbf{H}^H \right)^H \mathbf{H}_i \quad \text{(A.3)} \]

Appendix B: Derivation of the FD SF Semiblind Multiuser Equalizer

Substituting (8) into suboptimal FD SF semiblind
multiuser receiver with mixing parameter (17) and taking the expectation yields

$$J(f, \phi) = \phi \mathbb{E} \left[ \| f^H (H^T(j) + W(j)) c_p - b_p(j) \|^2 \right]$$

$$+ (1 - \phi) \mathbb{E} \left[ \| f^H (H^T(j) + W(j)) c_p^H - b_p(j) \|^2 \right].$$

Taking the gradient of (B.1) with respect to $f$ and setting to zero yields

$$\nabla_f J = \left( \sigma_1^2 H^H + \sigma_2^2 I \right) f - \left( A_p - \phi (A_p + A_d) \right) H_i = 0. \quad (B.2)$$

Hence, we obtain:

$$f = \left( A_p - \phi (A_p + A_d) \right) \left( \sigma_1^2 H^H + \sigma_2^2 I \right) H_i. \quad (B.3)$$

References


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